

High Performance Current Mode Controller

MAXIMUM RATING

Parameter	Symbol	Value	Unit
Supply Voltage (low impedance source)	V_i	30	V
Supply Voltage ($I_i < 30\text{mA}$)	V_i	Self Limiting	
Output Current	I_O	± 1	A
Output Energy (capacitive load)	EO	5	V
Analog Inputs (pins 2,3)		-0.3 to 6.3	mJ
Error Amplifier Output Sink Current		10	mA
Storage Temperature Range	T_{stg}	-65 to +150	$^{\circ}\text{C}$

* All voltages are with respect to pin 5, all currents are positive into the specified terminal.

ELECTRICAL CHARACTERISTICS ($V_{CC} = 15\text{V}$ (Note 2), $R_T = 10\text{K}$, $C_T = 3.3\text{nF}$, $T_A = T_{low}$ to T_{high} (Note 3) unless otherwise noted)

(Unless otherwise stated , these specifications apply for $0 < T_{amb} < 70^{\circ}\text{C}$; $V_i = 15\text{V}$ (Note 5), $R_T = 10\text{K}$, $C_T = 3.3\text{nF}$)

Parameter	Symbol	Test Conditions	PJ3844B / PJ3845B			Unit
			Min	Typ	Max	

REFERENCE SECTION

Output Voltage	V_{REF}	$I_o = 1\text{mA}, T_J = 25^{\circ}\text{C}$	4.90	5.00	5.10	V
Line Regulation	ΔV_{REF}	$12\text{V} < V_i < 25\text{V}$	-	6	20	mV
Load Regulation	ΔV_{REF}	$1 < I_o < 20\text{mA}$	-	6	25	mV
Temperature Stability (Note2)	$\Delta V_{REF} / \Delta T$		-	0.2	0.4	$\text{mV}/^{\circ}\text{C}$
Total Output Variation		Line, Load, Temperature(2)	4.82	-	5.18	V
Output Noise Voltage	V_n	$10\text{Hz} < f < 10\text{kHz}$ $T_J = 25^{\circ}\text{C}$ (2)	-	50	-	mV
Long Term Stability		$T_{amb} = 125^{\circ}\text{C}$, 1000Hrs(2)	-	5	25	mV
Output Short Circuit	Isc		-30	-100	-180	mA

OSCILLATOR SECTION

Initial Accuracy	f_s	$T_J = 25^{\circ}\text{C}$	47	52	57	KHz
Voltage Stability		$12 < V_i < 25\text{V}$	-	0.5	3	%
Temperature Stability		$T_{MIN} < T_{amb} < T_{MAX}$ (2)	-	5	-	%
Amplitude VPIN4 Peak to Peak	V_4		-	1.7	-	V

ERROR AMPLIFIER SECTION

Input Voltage ($V_o = 2.5\text{V}$)	V_2	$V_{PIN1} = 2.5\text{V}$	2.42	2.50	2.58	V
Input Bias Current	I_B		-	-0.3	-2.0	mA
	A_{VOL}	$2 < V_o < 4\text{V}$	65	90	-	dB
Unity Gain Bandwidth (2)	B		0.7	1.0	-	MHz
Supply Voltage Rejection	SVR		60	70	-	dB
Output Current Sink	I_{sink}	$V_{PIN2} = 2.7\text{V}, V_{PIN1} = 1.1\text{V}$	2.0	6	-	V
Output Current Source	I_{Source}	$V_{PIN2} = 2.3\text{V}, V_{PIN1} = 5\text{V}$	-0.5	-0.8	-	V
Output Voltage Swing High State	V_{OH}	$V_{PIN2} = 2.3\text{V}$, $R_L = 15\text{K}\Omega$ to Ground	4.55	4.85	-	V
Output Voltage Swing Low State	V_{OL}	$V_{PIN2} = 2.7\text{V}$, $R_L = 15\text{K}\Omega$ to Pin8	-	0.7	1.1	V

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Parameter	Symbol	Test Conditions	PJ3844B / PJ3845B			Unit
			Min	Typ	Max	

CURRENT SENSE SECTION

Current Sense Input Voltage Gain (Note 3 &4)	Gv		2.8	3.0	3.2	V/V
Maximum Input Signal	V ₃	V _{PIN1} =5V(Note 3)	0.9	1.0	1.1	V
Supply Voltage Rejection	SVR	12<Vi<25V(Note 3)	-	70	-	dB
Input Bias Current	I _B		-	-2.0	-10	mA
Delay to Output	T _d		-	150	300	ns

OUTPUT SECTION

Output Voltage						
Low State	V _{OL}	Isink=20mA	-	0.1	0.4	V
		Isink=200mA	-	1.5	2.2	
High State	V _{OH}	Isource=20mA	13	13.5	-	
		Isource=200mA	12	13.5	-	
Output Voltage Rise Time	tr	T _J =25°C, C _L =1.0nF (Note2)	-	50	150	ns
Output Voltage Fall Time	tf	T _J =25°C, C _L =1.0nF (Note2)	-	50	150	ns

UNDER-VOLTAGE LOCKOUT SECTION

Start-Up Threshold						
PJ3844B	V _{th}		14.5	16	17.5	V
PJ3845B			7.8	8.4	9.0	
Minimum Operating Voltage After Turn-On						
PJ3844B	V _{CC(min)}		8.5	10	11.5	V
PJ3845B			7.0	7.6	8.2	

PWM SECTION

Max. Duty Cycle	DCmax		44	48	50	%
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TOTAL STANDBY CURRENT

Start-Up Current	I _{st}		-	0.1	0.5	mA
Operating Supply Current	I _i	V _{PIN2} =V _{PIN3} =0V	-	11	20	mA
Zener Voltage	V _{iz}	I _i =25mA	30	34	-	V

Note:

1. Toggle flip flop used only in PJ3844 and PJ3845.
2. These parameters, although guaranteed, are not 100% tested in production.
3. Parameter measured at trip point of latch with V_{PIN2}=0
4. Gain defined as : $A = \frac{\Delta V_{PIN1}}{\Delta V_{PIN3}}$; $0 \leq V_{PIN3} \leq 0.8V$.
5. Adjust Vi above the start threshold before setting at 15V.

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FIGURE 1-TIMING RESISTOR versus OSCILLATOR FREQUENCY

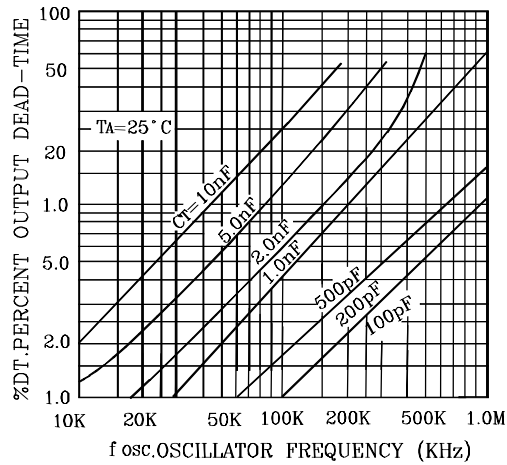


FIGURE 2-OUTPUT DEAD TIME versus OSCILLATOR FREQUENCY

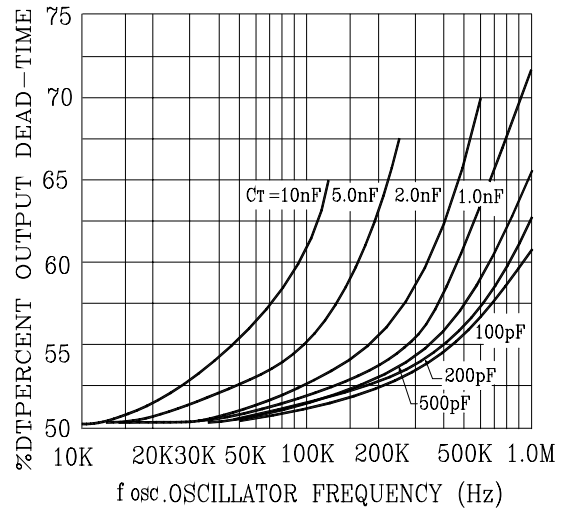


FIGURE 3-ERROR AMP SMALL SINGAL TRANSIENT RESPONSE

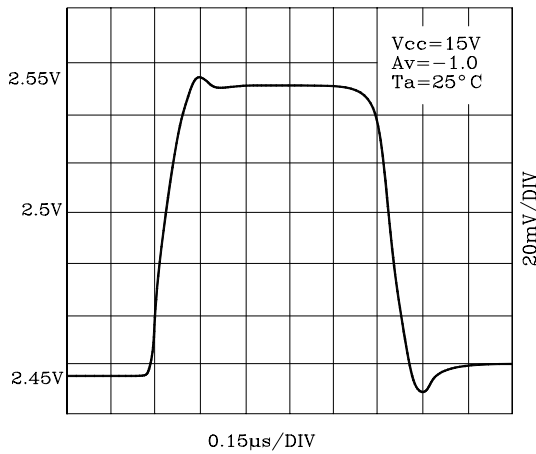


FIGURE 4-ERROR AMP LARGE RESPONSE TRANSIENT RESPONSE

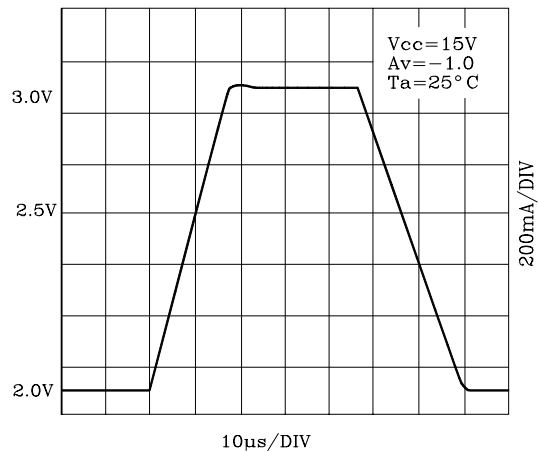


FIGURE 5-ERROR AMP OPEN-LOOP GAIN AND PHASE versus FREQUENCY

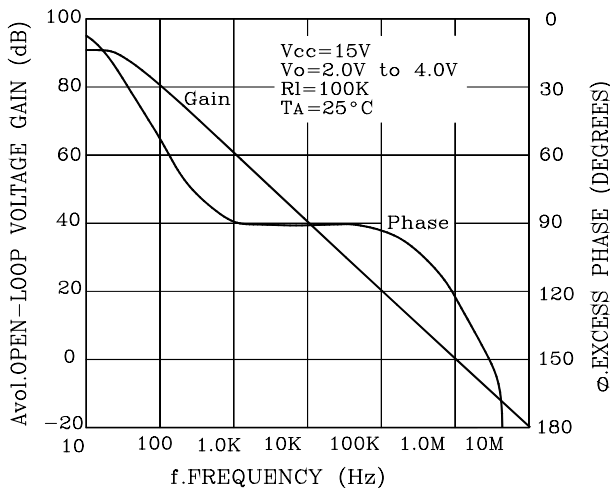
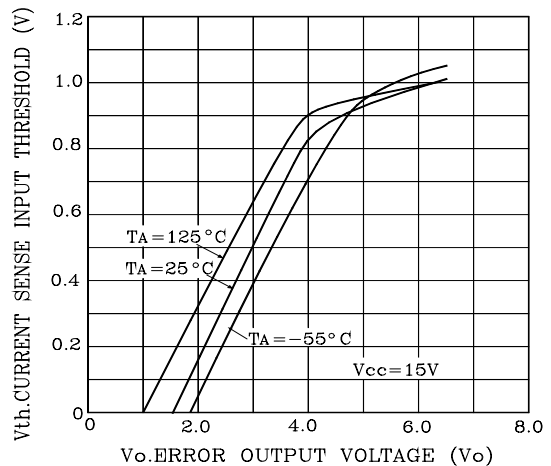


FIGURE 6-CURRENT SENSE INPUT THRESHOLD versus ERROR AMP OUTPUT VOLTAGE



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FIGURE 7-REFERENCE VOLTAGE CHANGE versus SOURCE CURRENT

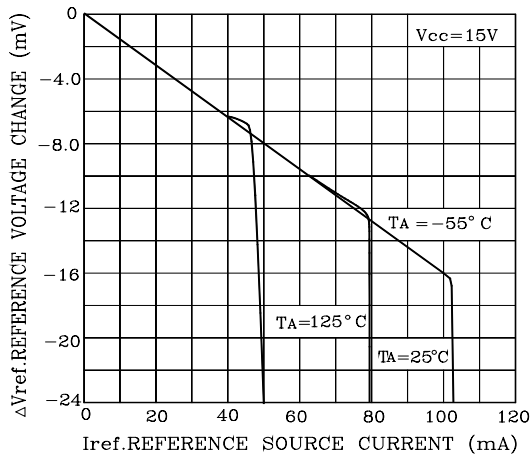


FIGURE 8-REFERENCE SHORT CIRCUIT CURRENT versus TEMPERATURE

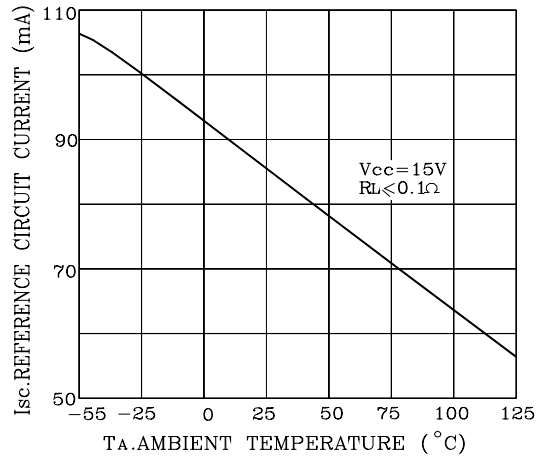


FIGURE 9-REFERENCE LOAD REGULATION

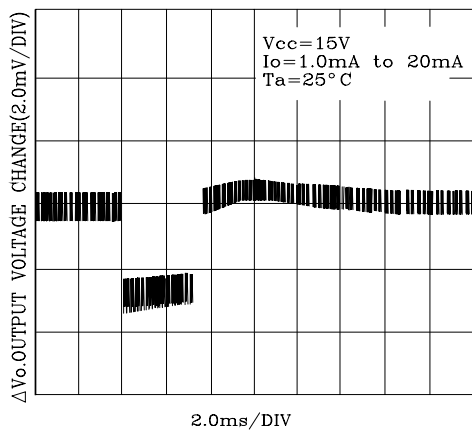


FIGURE 10-REFERENCE LINE REGULATION

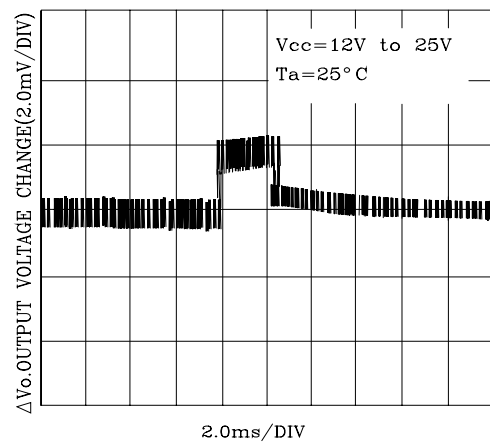


FIGURE 11- OUTPUT SATURATION VOLTAGE versus LOAD CURRENT

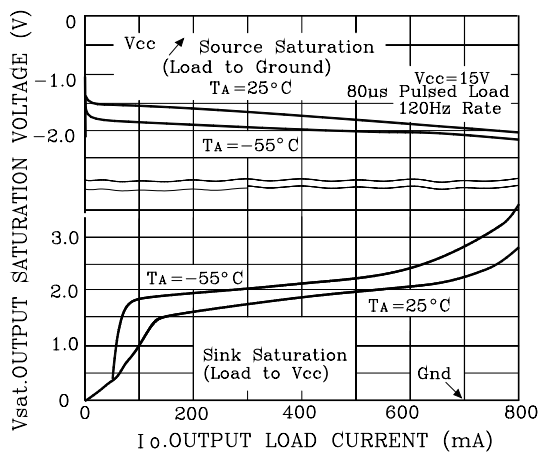
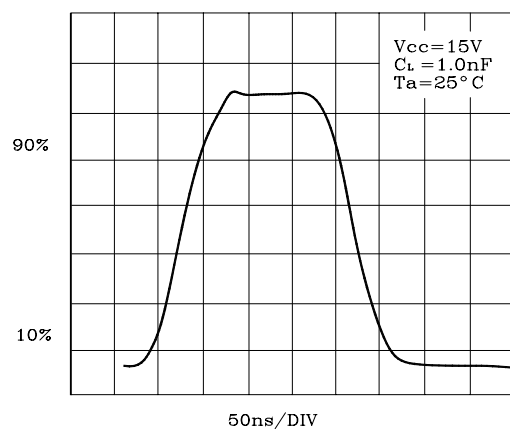


FIGURE 12-OUTPUT WAVEFORM



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FIGURE 13-OUTPUT CROSS CONDUCTION VOLTAGE

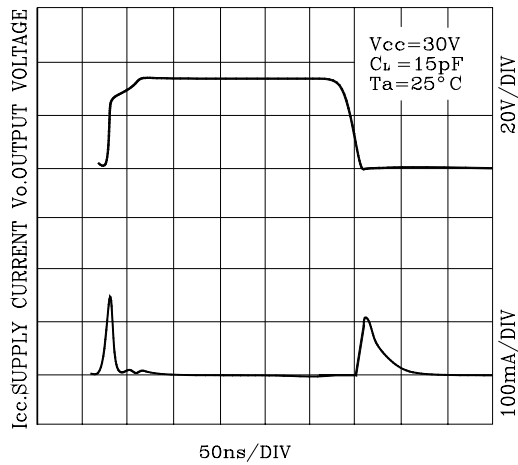
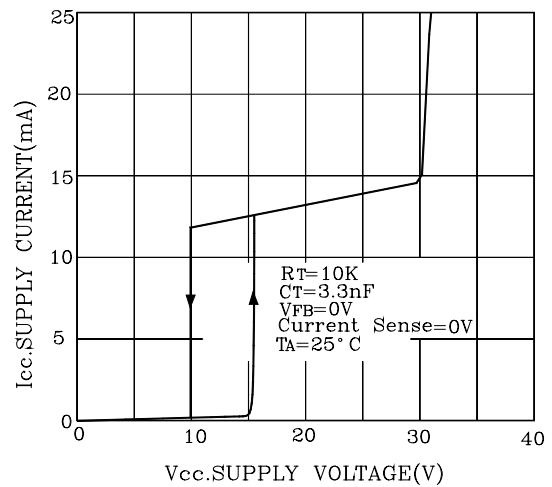


FIGURE 14-SUPPLY CURRENT versus SUPPLY VOLTAGE

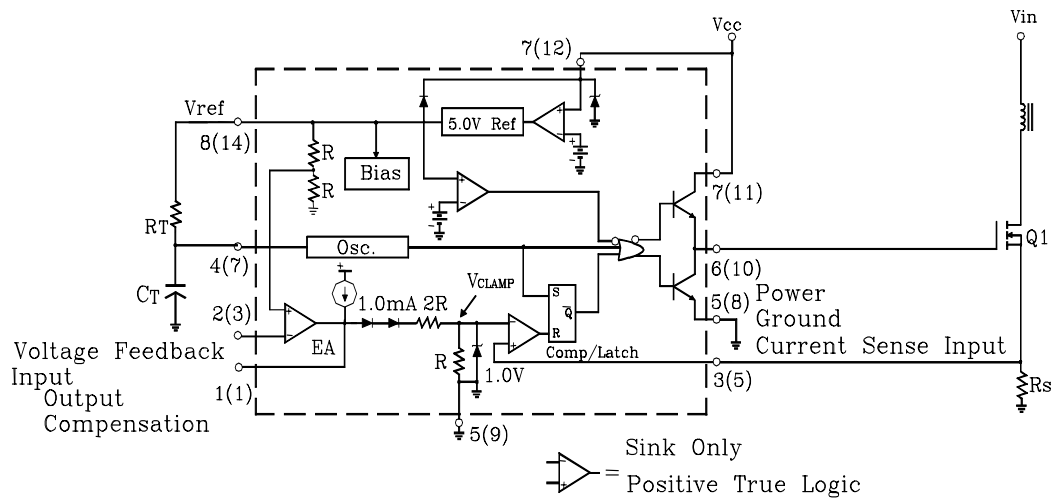


PIN FUNCTION DESCRIPTION

Pin No.	Function	Description
1	Compensation	This pin is the Error Amplifier output and is made available for loop compensation
2	Voltage Feedback	This is the inverting input of the Error Amplifier. It is normally connected to the switching power supply output through a resistor divider.
3	Current Sense	A voltage proportional to inductor current is connected to this input. The PWM uses this information to terminate the output switch conduction.
4	R_T/C_T	The Oscillator Frequency and maximum Output duty are programmed by connecting resistor R_T to V_{ref} and capacitor C_T to ground .Oscillator operation to 1.0MHz is possible.
5	Gnd	This pin is the combined control circuitry and power ground (8-pin package only).
6	Output	This output directly drives the gate of a power MOSFET.Peak current up to 1.0A are sourced and sunk by this pin.The output switches at one-half the oscillator frequency.
7	V_{cc}	This pin is the positive supply of the control IC.
8	V_{ref}	This pin is the reference output . It provides charging current for capacitor C_T through resistor R_T .

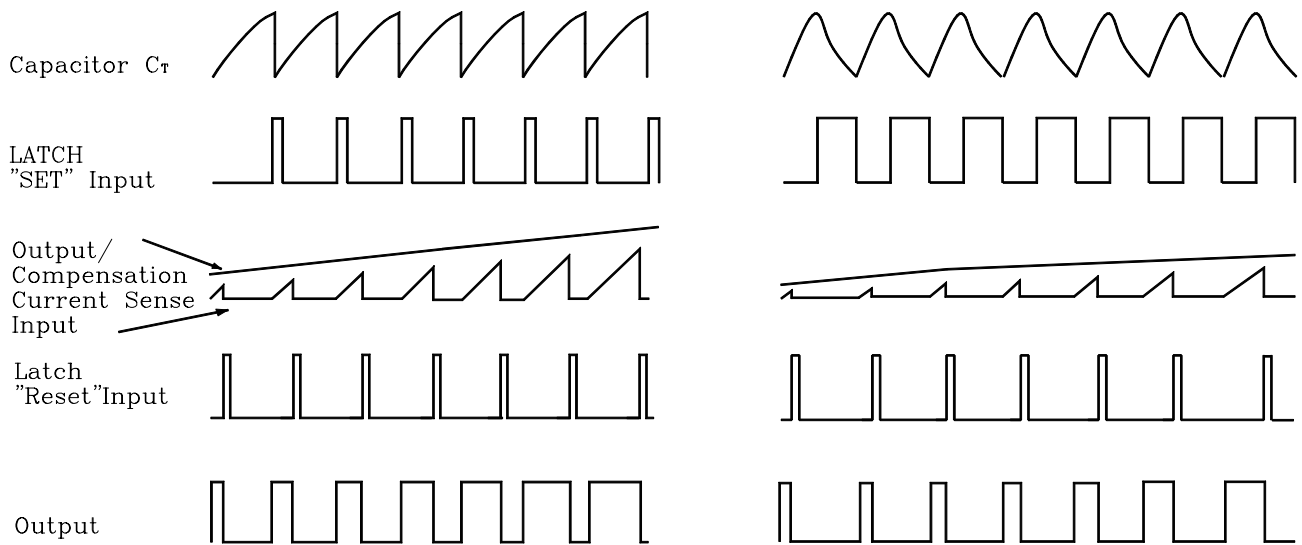
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FIGURE 17-REPRESENTATIVE BLOCK DIAGRAM



Pin numbers adjacent to terminals are for the 8 pin dual-in-line package.
Pin numbers in parenthesis are for the SOP-14 package.

FIGURE 18-TIMING DIAGRAM



UNDERVOLTAGE LOCKOUT

Two undervoltage lockout comparators have been incorporated to guarantee that the IC is fully functional before the output stage is enabled. The positive power supply terminal (V_{CC}) and the reference output (V_{ref}) are each monitored by separate comparators. Each has built-in hysteresis to prevent erratic output behavior as their respective thresholds are crossed. The V_{CC} comparator upper and lower thresholds are 1.84 V/7.6 V for the UC3845A

The V_{ref} comparator upper and lower thresholds are 3.6V/3.4V. The large hysteresis and low start-up current of the UC3844B makes it ideally suited in off-line converter applications where efficient bootstrap start-up technique (Figure 33). 36 V zener is connected as a shunt regulator from V_{CC} to ground. Its purpose is to protect the IC from excessive voltage that can occur during system start-up. The minimum operating voltage for the UC3844B is 11V.

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Output

These devices contain a single totem pole output stage that was specifically designed for direct drive of power MOSFET's. It is capable of up to $\pm 1.0A$ peak drive current and has a typical rise and fall time of 50 ns with a 1.0nF load. Additional internal circuitry has been added to keep the Output in a sinking mode whenever an undervoltage lockout is active. This characteristic eliminates the need for an external pull-down resistor.

The SOP-8 surface mount package provides separate pins for V_c (output supply) and Power Ground. Proper implementation will significantly reduce the level of switching transient noise imposed on the control circuitry. This becomes particularly useful when reducing the $I_{pk(max)}$ clamp level. The separate V_c supply input allows the designer added flexibility in tailoring the drive voltage independent of V_{cc} . A zener clamp is typically connected to this input when driving power MOSFETs in systems where V_{cc} is greater than 20V. Figure 25 shows proper power and control ground connections in a current sensing power MOSFET application.

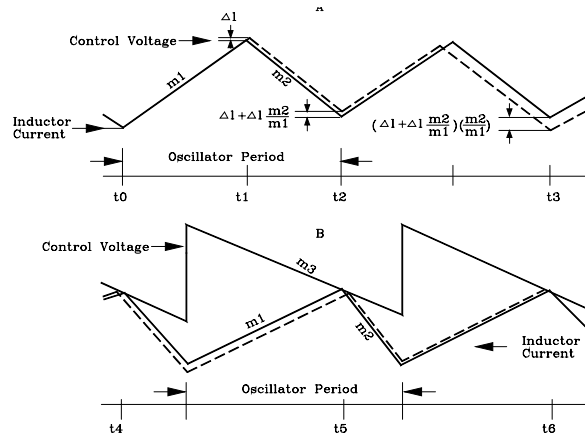
Reference

The 5.0V bandgap reference is trimmed to $\pm 2.0\%$ on the UC3844B. Its primary purpose to supply charging current to the oscillator timing capacitor. The reference has short circuit protection and is capable of providing in excess of 20mA for powering additional control system circuitry.

Design Considerations

Do not attempt to construct the converter on wirewrap or plug-in prototype boards. High frequency circuit layout techniques are imperative to prevent pulsewidth jitter. This is usually caused by excessive noise pick-up imposed on the Current Sense or Voltage Feedback inputs. Noise immunity can be improved by lowering circuit impedances at these points. The printed circuit layout should contain a ground plane with lowcurrent signal and high-current switch and output grounds returning separate paths back to the input filter capacitor. Ceramic bypass capacitors ($0.1 \mu F$) connected directly to V_{cc} , V_c , and V_{ref} may be required depending upon circuit layout. This provides a low impedance path for filtering the high frequency noise. All high current loops should be kept as short as possible using heavy copper runs to minimize radiated EMI. The Error Amp compensation circuitry and the converter output voltage divider should be located close to the IC and as far as possible from the power switch and other noise generating components.

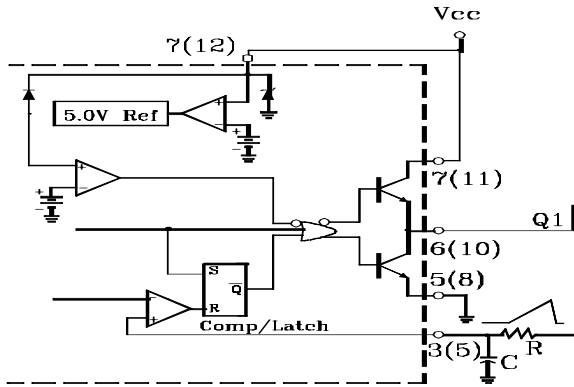
FIGURE 19-CONTINUOUS CURRENT WAVEFORMS



Current mode converters can exhibit subharmonic oscillations when operating at a duty cycle greater than 50% with continuous inductor current. This instability is independent of the regulators closed loop characteristics and is caused by the simultaneous operating conditions of fixed frequency and peak current detecting. Figure 19A shows the phenomenon graphically. At t_0 , switch conduction begins, causing the inductor current to rise at a slope of m_1 . This slope is a function of the input voltage divided by the inductance. At t_1 , the Current Sense Input reaches the threshold established by the control voltage. This causes the switch to turn off and the current to decay at a slope of m_2 , until the next oscillator cycle. This unstable condition can be shown if a perturbation is added to the control voltage, resulting in a small ΔI (dashed line). With a fixed oscillator period, the current decay time is reduced, and the minimum current at switch turn-on (t_2) is increased by $\Delta I + \Delta I \frac{m_2}{m_1}$. The minimum current at the next cycle (t_3) decreases to $(\Delta I + \Delta I \frac{m_2}{m_1})(\frac{m_2}{m_1})$. This perturbation is multiplied by $\frac{m_2}{m_1}$ on each succeeding cycle, alternately increasing and decreasing the inductor current at switch turn-on. Several oscillator cycles may be required before the inductor current reaches zero causing the process to commence again. If $\frac{m_2}{m_1}$ is greater than 1, the converter will be unstable. Figure 19B shows that by adding an artificial ramp that is synchronized with the PWM clock to the control voltage, the ΔI perturbation will decrease to zero on succeeding cycles. This compensating ramp (m_3) must have a slope equal to or slightly greater than $\frac{m_2}{2}$ for stability. With $\frac{m_2}{2}$ slope compensation, the average inductor current follows the control voltage yielding true current mode operation. The compensating ramp can be derived from the oscillator and added to either the Voltage Feedback or Current Sense inputs (Figure 32).

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FIGURE 26-CURRENT WAVEFORM SPIKE SUPPRESSION



The addition of RC filter will eliminate instability caused by the leading edge splik on the current waveform.

FIGURE 27-MOSFET PARASITIC OSCILLATIONS

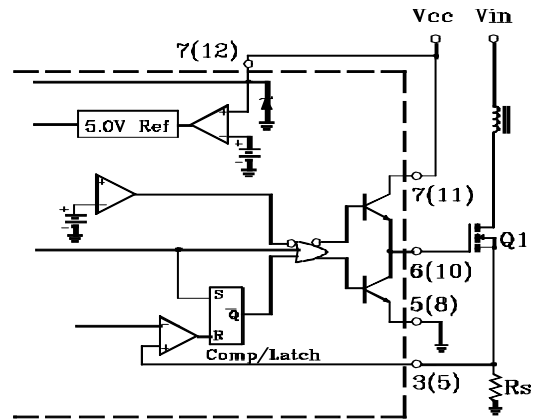
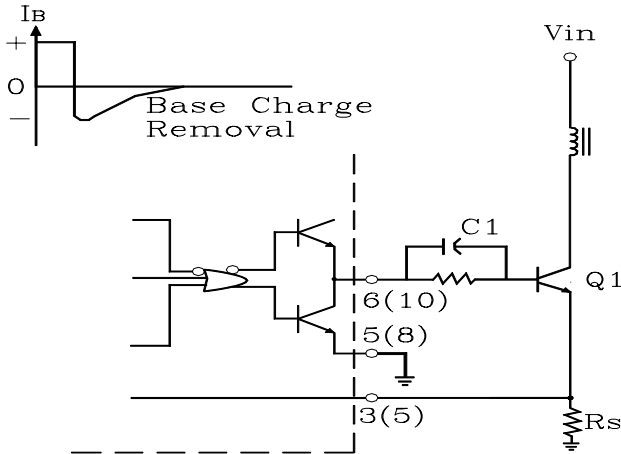


FIGURE 28-BIPOLAR TRANSISTOR DRIVE



The totem-pole output can furnish negative base current for enhanced transistor turn-off,with the additions of capacitor C1.

FIGURE 29-ISOLATED MOSFET DRIVE

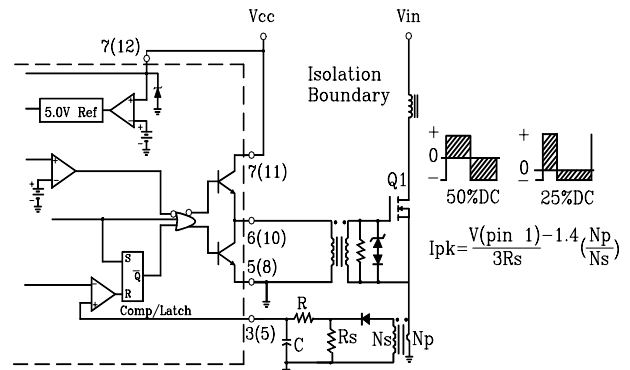
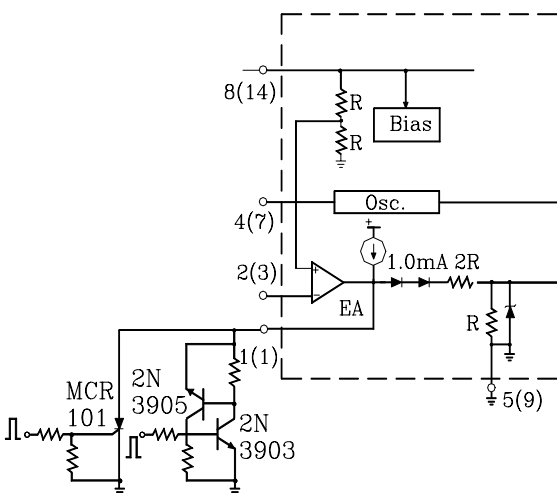
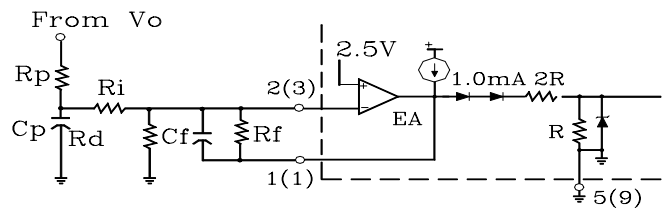


FIGURE 30-LATCHED SHUTDOWN

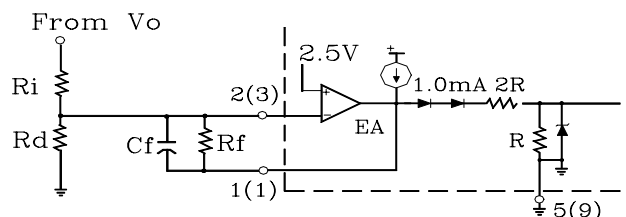


The MCR101 SCR must be selected for a holding of less than 0.5mA at T_A (min).The simple two transistor circuit can be used in place of the SCR as shown.All resistors are 10K.

FIGURE 31-ERROR AMPLIFIER COMPENSATION



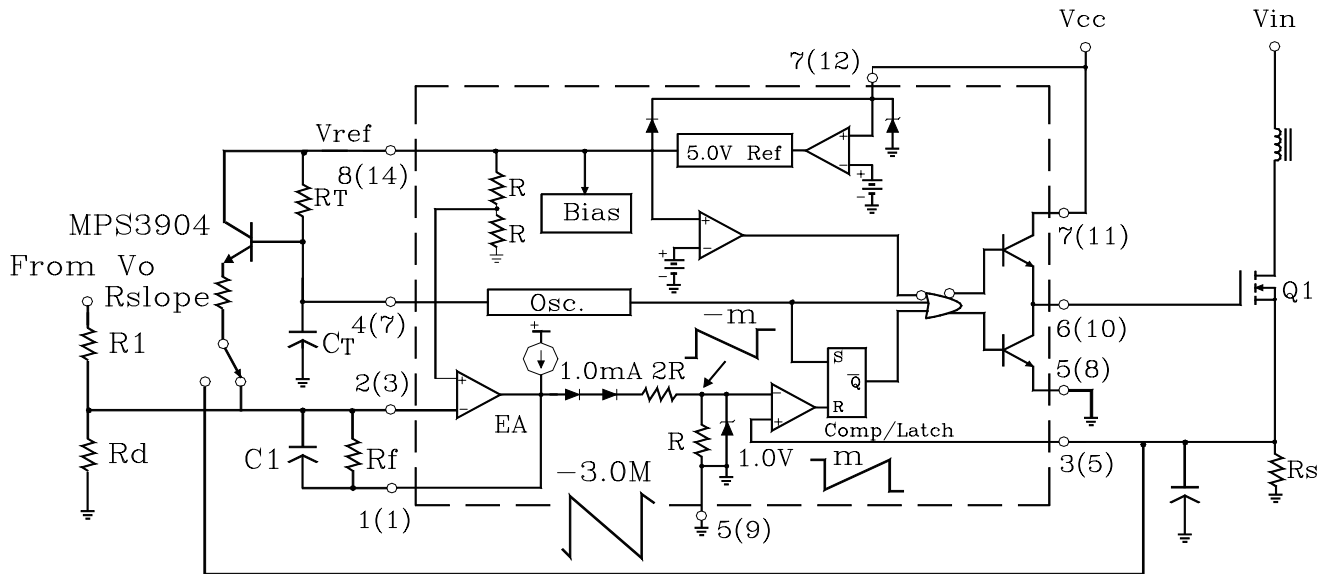
Error Amp compensation circuit for stabilizing any currentmode topology except for boost and flyback converters operating with continuous inductor current.



Error Amp compensation circuit for stabilizing any currentmode topology except for boost and flyback converters operating with continuous inductor current.

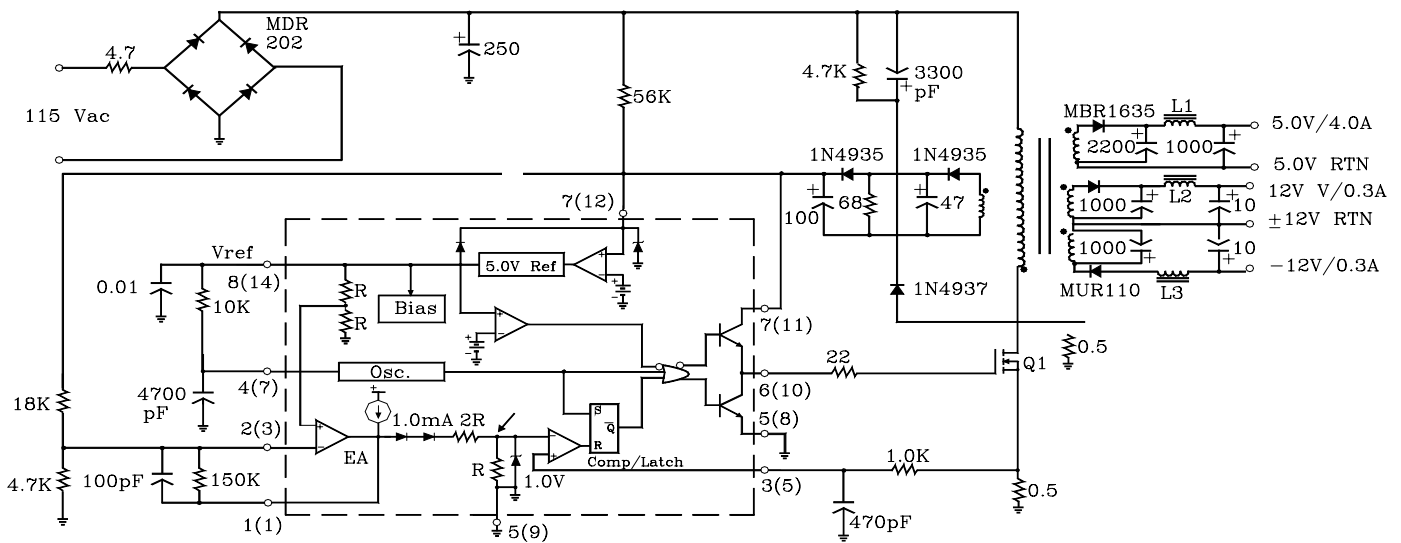
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FIGURE 32-SLOPE COMPENSATION



The buffered oscillator ramp can resistively summed with either the voltage feedback or current sense inputs to provide slope compensation.

FIGURE 33-27 WATT OFF-LINE REGULATION



T1-Primary:45 Turns #26 AWG

Secondary ±12V :9 Turns #30 AWG (2 strands) Bifiliar Wound

Secondary 5.0V: 4 Turns (six strands) #26 Hexfiliar Wound

Secondary Feedback : 10 Turns #30 AWG (2 strands) Bifiliar Wound

Core: Ferroxcube EC35-3C8

Bobbin : Ferroxcube EC35PCB1

Gap : ≅ 0.10" for a primary inductance of 1.0mH

L1-15 μH at 5.0A, Coilcraft 27156.

L2.L3-25 μH at 1.0A, Coilcraft 27157.

Line Regulation : 5.0V ±12V	Vin=95 to 130 Vac	=50mV or ±0.5% =24mV or ±0.1%
Load Regulation : 5.0V ±12V	Vin=115Vac, Iout =1.0A to 4.0A Vin=115Vac,Iout=100mA to 300mA	=300mV or ±3.0% =60mV or ±0.25%
Output Ripple : 5.0V ±12V	Vin=115Vac	40mVp-p 80 Vp-p
Efficiency	Vin=115Vac	70%

All outputs are at nominal load currents unless otherwise noted.

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OPERATING DESCRIPTION

The UC3844B series are high performance, fixed frequency, current mode controllers, They are specifically designed for Off-Line and DC-to-DC converter applications offering the designer a cost effective solution with minimal external components . A representative block diagram is shown in Figure 17.

OSCILLATOR

The oscillator frequency is programmed by the values selected for the timing components R_T and C_T . Capacitor C_T is charged from the 5.0V reference through resistor R_T to approximately 2.8V and discharge to 1.2V by an internal current sink. During the discharge of C_T , the oscillator generates an internal blanking pulse that holds the center input of the NOR gate high. This causes the Output to be in a low state, thus producing a controlled amount of output deadtime. Figure 1 shows R_T versus Oscillator Frequency and Figure 2, Output Deadtime versus Frequency, both for given values of C_T . Note that many values of R_T and C_T will give the same oscillator frequency but only onne combination will yield a specific output deadtime at a given frequency. The oscillator thresholds are temperature compensated, and the discharge current is trimmed and guaranteed to within $\pm 10\%$ at $T_J = 25^\circ\text{C}$. These internal circuit refinements minimum variations of oscillator frequency and maximum output duty cycle. The results are shown in Figure 3 and 4.

In many noise sensitive applications it may be desirable to frequency-lock the converter to an external system clock. This can be accomplished by applying a clock signal to the circuit shown in Figure 20. For reliable locking. The free-running oscillator frequency should be set about 10% less than the clock frequency . A method for multi unit synchronization is shown in Figure 21. By tailoring the clock waveform, accurate Output duty cycle clamping can be achieved.

ERROR AMPLIFIER

A fully compensated Error Amplifier with access to the inverting input and output is provided. It features a typical DC voltage gain of 90dB, and a unity gain bandwidth of 1.0MHz with 57 degrees of phase margin (Figure 7). The non-inverting input is internally biased at 2.5V and is not pinned out. The converter output voltage is typically divided down and monitored by the inverting input. The maximum input bias current is $-2.0\mu\text{A}$ which can cause an output voltage error that is equal to the product of the input bias current and the equivalent input divider source resistance.

The Error Amp Output (Pin 1) is provided for external loop compensation (Figure 31). The output voltage is offset by two diode drops ($\approx 1.4\text{V}$) and divided by three before it connects to the inverting input of the Current Sense Comparator. This guarantees that no drive pulses appear at the Output (Pin 6) when Pin 1 is at its lowest state (V_{OL}). This occurs when the power supply is operating and the load is removed, or at the beginning of a soft-start interval (Figure 23,24). The Error Amp minimum feedback resistance is limited by the amplifier's source current (0.5mA) and the required output voltage (V_{OH}) to reach the comparator's 1.0V clamp level:

$$R_{f(\text{MIN})} = [3.0 (1.0\text{V}) + 1.4\text{V}] / 0.5\text{mA} = 8800\Omega$$

CURRENT SENSE COMPARATOR AND PWM LATCH

The UC3844B operate as a current mode controller, whereby output switch conduction is initiated by the oscillator and terminated when the peak inductor current reaches the threshold level established by the Error Amplifier Output/Compensation (Pin 1). Thus the error signal controls the peak inductor current on a cycle-by-cycle basis. The Current Sense Comparator PWM Latch configuration used ensures that only a single appears at the Output during any given oscillator cycle. The inductor current is converted to a voltage by inserting the ground referenced sense resistor R_S in series with the source of output switch Q1. This voltage is monitored by the Current Sense Input (Pin 3) and compared to a level derived from the Error Amp Output. The peak inductor current under normal operating conditions is controlled by the voltage at pin 1 where:

$$I_{PK} = [V(\text{Pin 1}) - 1.4\text{V}] / 3R_S$$

Abnormal operating conditions occur when the power supply output is overloaded or if output voltage sensing is lost, Under these conditions, the Current Sense Comparator threshold will be internally clamped to 1.0V. Therefore the maximum peak switch current is:

$$I_{PK(\text{MAX})} = 1.0\text{V} / R_S$$

When designing a high power switching regulator it becomes desirable to reduce the internal clamp voltage in order to keep the power dissipation of R_S to a reasonable level. A simple method to adjust this voltage is shown in Figure 22. The two external diodes are used to compensate the internal diodes yielding a constant clamp voltage over temperature. Erratic operation due to noise pickup can result if there is an excessive reduction of the $I_{PK(\text{max})}$ clamp voltage.

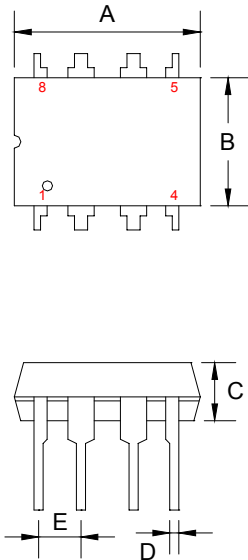
A narrow spike on the leading edge of the current waveform can usually be observed and may cause the power supply to exhibit an instability when the output is lightly loaded. This spike is due to the power transformer interwinding capacitance and output rectifier recovery time. The addition of an RC filter on the Current Sense Input with a time constant that approximates the spike duration will usually eliminate the instability: refer to Figure 26.

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DIP-8 Mechanical drawing

1.Top View

2.Side View

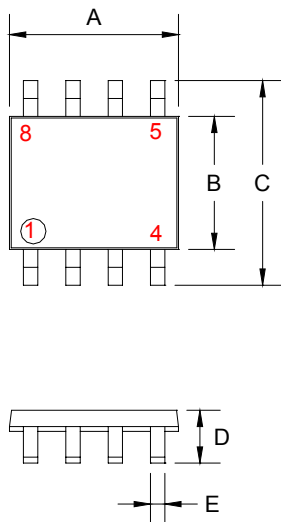


DIP-8 DIMENSION				
DIM	MILLIMETERS		INCHES	
	MIN	MAX	MIN	MAX
A	8.85	9.05	0.348	0.356
B	6.30	6.40	0.248	0.252
C	3.65	3.95	0.143	0.156
D	0.45	0.55	0.017	0.022
E	2.54BSC		0.10BSC	
F	7.75	8.00	0.305	0.315
G	0.20	0.30	0.007	0.012
H	-	10°	-	10°

SOP-8 Mechanical drawing

1.Top View

2.Side View



SOP-8 DIMENSION				
DIM	MILLIMETERS		INCHES	
	MIN	MAX	MIN	MAX
A	4.80	5.00	0.189	0.197
B	3.80	4.00	0.150	0.157
C	5.80	6.20	0.228	0.244
D	1.40	1.50	0.055	0.059
E	0.33	0.51	0.013	0.020
F	1.27BSC		0.05BSC	
G	0.19	0.25	0.007	0.010
H	0.40	1.27	0.016	0.050
θ	0°	8°	0°	8°